

# Intelligent control of induction motor without speed sensor

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## ABSTRACT

This paper presents a proposed sensorless algorithm for induction motor (IM) speed control based on artificial neural networks (ANNs). The Indirect rotor field oriented (IRFO) technique is applied to control the motor. It is designed based on the proportional integral (PI) controller. The particle swarm optimization (PSO) algorithm is used as a good solution for the problems associated with the design of the proportional integral (PI) controller gains. The PSO is compared with the conventional methods. The proposed controller (PSO-PI) is then integrated with the artificial neural network (ANN) speed estimator. The MATLAB/Simulink is used for the simulation of the system. The obtained simulation results for the proposed technique are very close to the actual ones.

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## 1. INTRODUCTION

The induction motors (IMs) are considered the horsepower of industry. They have many advantages compared to other types. Therefore, they are used in large sections due to the simple construction design, ruggedness and low maintenance. Unfortunately, their speed controller design is considered a great challenge due to the nonlinearity of motor model [1].

Several techniques are used to control the IM. These techniques can be classified as scalar control or volts/hertz (V/f) [2] and vector control which can be classified into field oriented control (FOC) [3] and direct torque control (DTC) [4]. Most of the drives have employed vector control especially FOC techniques for the last three decades thanks to their advantage compared to V/f and DTC methods. The controller based on the V/f and DTC cannot realize the desired performance through transient operation since they consider the motor model in steady state [1], [5]. The classical DTC performance also degraded especially for low speed operating conditions because it has variable switching frequency high ripples in flux and torque [6]. The FOC techniques have a great attention, since it solves the problems of other controllers and make the speed control of IM as of separately excited DC-motors [5]. The IRFOC [7], [8] is the most widely used because of its insensitivity to the stator resistance change.

Classical proportional integral (PI) is a simple linear controller which can achieve IM control based on the FOC phenomena. Though, the PI controller has main drawbacks such as the mismatch between the model parameters and the actual model and un-modeled and nonlinear dynamics [8], these troubles make the tuning process of the controller is difficult and may cause instability in the system. There are many researches to overcome the problems of conventional selection of PI controller gains ( $K_p$ ,  $K_i$ ) which depend on using Artificial Intelligent (AI) techniques such as particle swarm optimization (PSO) and genetic

algorithm (GA) [9]-[13]. Tista Banerjee, Sumana Chowdhuri, Gautam Sarkar, *et al.*, [14] introduces a comparison between Zigler-Nichol method and the AI (GA and PSO). The comparison of their results shows the better of both AI techniques than Zigler-Nichol one but the PSO has better performance such as simplicity, minimizing the computational time and it has stable convergence characteristics compared to GA. In this paper the PSO is selected to make tuning of PI gains.

The approach of speed sensorless controls for IMs have been getting more interest in different industrial applications because they can make cost reduction and evade the problems associated with the mechanical speed sensors. Also, they remove the installing difficulty of the speed sensors in some applications [15], [16]. There are different techniques for estimating the IM speed and its rotor flux. These techniques can be classified as, (i) signal injection methods [16], the main drawbacks of these techniques are the causing of torque ripples, vibration and audible noise. Furthermore, motors having low saliency content do not give an appreciable response, (ii) open loop speed estimation techniques, there are two main techniques voltage or stator model and current or rotor model [17]. These approaches depend heavily on the motor parameters, (iii) model reference adaptive system (MRAS) [18], this method has the integration problem which may lead the system to instability, (iv) full order and reduced order closed loop observers. There are many approaches for these techniques, such as adaptive observer [19] which uses a complex gain in the feedback signal, sliding mode observer (SMO) [20], which has chattering carried out due to the high switching gain. Extended Kalman filter EKF has been proposed in [21] as a solution for better flux estimation. These approaches contain some inherent disadvantages such as highly computational processes [20], (v) artificial intelligent (AI) methods like artificial neural networks (ANNs) and fuzzy logic (FL) [22]-[24]. These techniques have a great attention in the last decades in many fields especially pattern recognition and control systems since they can deal with the complex or non-linear process without the needing for the relations between the input and output [25]. The FL was employed with MRAS in [21]. The ANN technique used with MRAS in [23]. The results were good but still depend on the motor parameters and lost the basic advantage of the AI techniques which make them more adequate to deal with the system with parameters independently.

This paper introduces a new technique for IRFOC of IM using ANN technique as a speed estimator. The proposed technique estimates the motor speed independently of the motor parameters and equations this make the proposed system more robust and unaffected to the motor parameter variations. The system efficient improved using PSO to calculate the controller gains directly from the system.

This paper is organized as follows. The mathematical model of IM is presented in Section 2. Section 3 presents the conventional- and the proposed PSO- PI controllers for speed control of IM based on IRFOC. In Section 4, the speed estimator based on the ANN technique is evaluated., the simulation results using MATLAB/Simulink are presented for different operating conditions to validate the efficiency of the proposed sensorless technique in in Section 5. Finally, some conclusions are presented in Section 6.

## 2. INDUCTION MOTOR MODELING

A three- phase, squirrel cage IM is considered in this paper. The d-q reference frame model of the IM can be represented as [18].

$$\frac{d}{dt} \begin{bmatrix} i_{ds} \\ i_{qs} \\ \lambda_{dr} \\ \lambda_{qr} \end{bmatrix} = \begin{bmatrix} -a_1 & \omega_e & a_2 & Pa_3 \omega_r \\ -\omega_e & -a_1 & -Pa_3 \omega_r & a_2 \\ a_5 & 0 & -a_4 & \omega_{sl} \\ 0 & a_5 & -\omega_{sl} & -a_4 \end{bmatrix} \begin{bmatrix} i_{ds} \\ i_{qs} \\ \lambda_{dr} \\ \lambda_{qr} \end{bmatrix} + \begin{bmatrix} c & 0 \\ 0 & c \\ 0 & 0 \\ 0 & 0 \end{bmatrix} \begin{bmatrix} V_{ds} \\ V_{qs} \end{bmatrix} \quad (1)$$

where,  $a_1 = \frac{1}{\sigma l_s} (R_s + R_r \frac{l_m^2}{l_r^2})$ ,  $a_2 = \frac{1}{\sigma l_s} (R_r \frac{l_m}{l_r^2})$ ,  $a_3 = \frac{1}{\sigma l_s} \frac{l_m}{l_r}$ ,  $a_4 = \frac{R_r}{l_r}$ ,  $a_5 = \frac{R_r l_m}{l_r}$ ,  $c = \frac{1}{\sigma l_s}$ ,  $\sigma = 1 - \frac{l_m^2}{l_r l_s} =$  leakage coefficient and  $\omega_{sl} = \omega_e - P\omega_r =$  Slip frequency (speed).

$V_{ds}, V_{qs}$ : d-and q- axis stator voltages (V),  $I_{ds}, I_{qs}$ : d-and q- axis stator currents (A),  $R_s, R_r$ : Stator and rotor resistances ( $\Omega$ ),  $L_s, L_r, L_m$ : Stator self, rotor self and mutual inductances (H),  $P$ : Number of poles pairs,  $\lambda_{ds}, \lambda_{qs}$ : d-and q- axis stator fluxes (Wb),  $\lambda_{dr}, \lambda_{qr}$ : d- and q- axis rotor fluxes (Wb),  $\omega_e, \omega_r, \omega_{sl}$ : Synchronous, rotor, slip speed (rad/s). The electromagnetic developed torque of the IM can be expressed as.

$$T_e = \frac{3}{2} \frac{Pl_m}{l_r} (\lambda_{dr} i_{qs} - \lambda_{qr} i_{ds}) \quad (2)$$

The mechanical of IM.

$$\dot{\omega}_r = \frac{1}{J} (T_e - B\omega_r - T_l) \quad (3)$$

where,  $T_l$ : load torque (Nm),  $B$ : Coefficient of viscous friction (Nm.s/rad),  $J$ : Moment of inertia (kg.m<sup>2</sup>).

### 3. PI CONTROL DESIGN

Since the PI controllers are widely used in IM drives and proved to be simple and effective. A PI controller is designed to control the IM speed as illustrated in Figure.1. Based on the IRFOC principle, the stator current component of the flux ( $i_{ds}$ ) is aligned with the direction of flux of the rotor ( $\lambda_r$ ) and the stator current of the torque ( $i_{qs}$ ) is aligned with the vertical direction to it as shown in Figure 2, for this situation:

$$\lambda_{qr} = 0, \dot{\lambda}_{qr} = 0, \lambda_{dr} = \lambda_r = \text{rotor flux} \quad (4)$$

then, the electromagnetic developed torque (2) can be reduced to the next equation:

$$T_e = \frac{3}{2} \frac{P l_m}{l_r} (\lambda_{dr} i_{qs}) = K_t \lambda_{dr} i_{qs} \quad (5)$$

$$\text{with } K_t = \frac{3}{2} \frac{P l_m}{l_r}$$

Considering the field orientation condition, the dynamic model of the IM becomes.

$$\frac{d}{dt} \begin{bmatrix} i_{ds} \\ i_{qs} \\ \lambda_{dr} \end{bmatrix} = \begin{bmatrix} -a_1 & \omega_e & a_2 \\ -\omega_e & -a_1 & -P a_3 \omega_r \\ a_5 & 0 & -a_4 \end{bmatrix} \begin{bmatrix} i_{ds} \\ i_{qs} \\ \lambda_{dr} \end{bmatrix} + \begin{bmatrix} c & 0 \\ 0 & c \\ 0 & 0 \end{bmatrix} \begin{bmatrix} V_{ds} \\ V_{qs} \end{bmatrix} \quad (6)$$

From (4) to (6), the relations can be obtained:

$$i_{qr} = -\frac{L_m}{L_r} i_{qs} \quad (7)$$

$$\lambda_{dr} = \frac{L_m}{1+T_r p} i_{ds} \quad (8)$$

$$\omega_{sl} = \frac{L_m}{T_r \lambda_{dr}} i_{qs} \quad (9)$$

In the steady state,  $\lambda_{dr} = L_m i_{ds}$  and  $i_{dr} = 0$ . To ensure the field orientation concept, the controller consists of three PI loops to control three interactive variables independently ( $\lambda_r, T_e, \omega_r$ ). The following two methods are illustrated for tuning the PI gains.

#### 3.1. Conventional method

The IM can be represented by a simple model as shown in Figure1 depending (3) [27]. The whole equation for the closed-loop system is.

$$\frac{\omega_r}{\omega_r^*} = \frac{K_\omega K_p S + K_\omega K_i}{\tau_\omega S^2 + (1 + K_\omega K_p) S + K_\omega K_i} \quad (10)$$

where,  $K_\omega = \frac{P}{B}$  is the motor gain,  $\tau_\omega = \frac{J}{B}$ , is mechanical time constant.

Assume a first order system for the (10) which can be presented by (11).

$$\frac{\omega_r}{\omega_r^*} = \frac{1}{\tau_c S + 1} \quad (11)$$

where,  $\tau_c$  is the closed-loop time constant of the system.

Solving (10) and (11) lead to the following parameters for the PI controller.

$$K_p = \frac{\tau_\omega}{K_\omega \tau_c}, K_i = \frac{1}{K_\omega \tau_c} \quad (12)$$

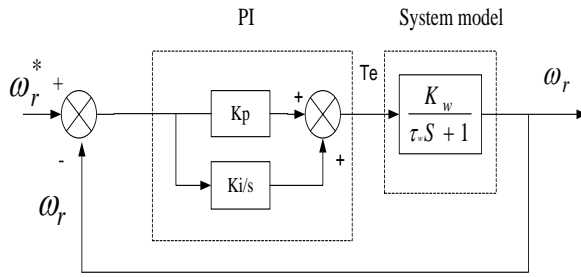


Figure 1. Closed loop PI controller

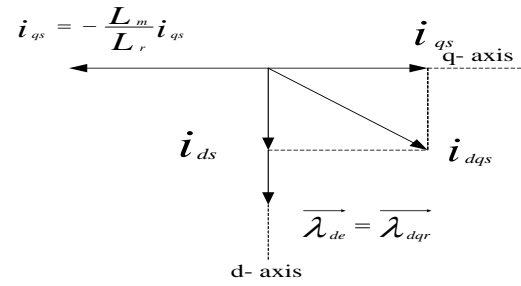


Figure 2. Phasor diagram of a field oriented IM

The (12) computes the PI controller parameters as a function of the mechanical time constant and the closed-loop time constant. This method has its disadvantages, it deals with the mechanical part of the system and doesn't take into account the effect of the inner control loops, so it needs to make an agree between outer and inner control loops, also it depends on try and error to get the best solution for different cases.

### 3.2. Self-tuning PI controller

Conventional control depends on using the mathematical model to control the system. When there are environmental disturbances or variations on the system parameters, these make the system performance is not fitting and diverges from the desired act. Furthermore, of the system mathematical model usual computations are difficult because the IM equations are complex and nonlinear dependent. This reduces the reliability of the system under control. To overcome these problems the tuning of the PI gains is done using PSO. The arrangement of the PSO algorithm with the PI controller is shown in Figure 3.

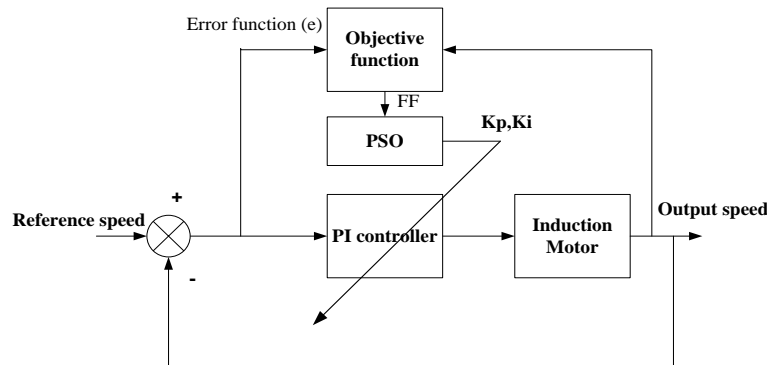


Figure 3. PSO algorithm with PI controller

The PSO algorithm is put directly in parallel with the simulated model, where it evaluates the PI gains according to a proposed fitness or objective function and its inherent structure. The design of PSO algorithm can be considered as a searching algorithm in which a group of particles ( $i$ ) are searching the target position in parallel and every iteration they update their position according to the global best results. The particle  $i$  position can be improved by (13) [10]-[12].

$$S_i^{k+1} = S_i^k + V_i^{k+1} \quad (13)$$

where,  $S_i^k$  is the previous position and  $V_i^{k+1}$  is the new velocity which can be evaluated by (14) [12].

$$V_i^{k+1} = C(wV_i^k + (c_1r_1(pbest_i - S_i^k)) + c_2r_2(gbest_i - S_i^k)) \quad (14)$$

where,  $V_i^k$  is particle  $i$  previous velocity for iteration  $k$ ,  $r_1$  and  $r_2$  are random numbers, usually between (0, 1),  $pbest$  is the particle  $i$  local best position,  $gbest$  is the particle  $i$  global best position,  $c_1$  is cognitive parameter

and  $c_2$  is social parameter and they must have a positive values,  $w$  is weight function of the particle velocity. For fast convergence, it's recommended to use a varied value for the weight  $w$  starting from a high value and then decreased gradually to reach zero at the end of iteration process. Finally,  $C$  is a constriction factor which used to get better choice of the parameters. The PSO has procedure, a) generate particles initial position, b) evaluate particles searching points using (13), c) modify particles searching points using (14), and d) repeat until reach the target or maximum iterations.

The proper choice of the fitness function is essential to get better performance. There are different essential standards which can be used as fitness function, more details in [6]-[8]. Integrated of time weight absolute error (ITAE) is one of the best standard formula which can be used as fitness function. Though, it is time dependent which mean it doesn't give the desired solution for small time operation. To overcome this problem, the absolute value of the overshoot in the tracked speed is considered with the ITAE function as.

$$FF = ITAE + |\text{overshoot}|. \quad (15)$$

where,

$$ITAE = \int_0^{\infty} t|e(t)|dt \quad (16)$$

#### 4. ANN SENSORLESS BASED TECHNIQUE

The ANN can be described as a set of neurons that are connected in and organized in several layers [23] as shown in Figure 4. In this paper a Feedforward Neural Network (FFNN) is applied for speed estimation the IM motor. It's simple and fast compared to other types since it does not need a feedback signal. Then this estimator is used as a feedback signal to the controller instead of the actual one. The input signals of the ANN are changed consistent with the correlation weights. The error between chosen outputs and outputs of the ANN is minimized in the ANN learning process by updating the connection weights.

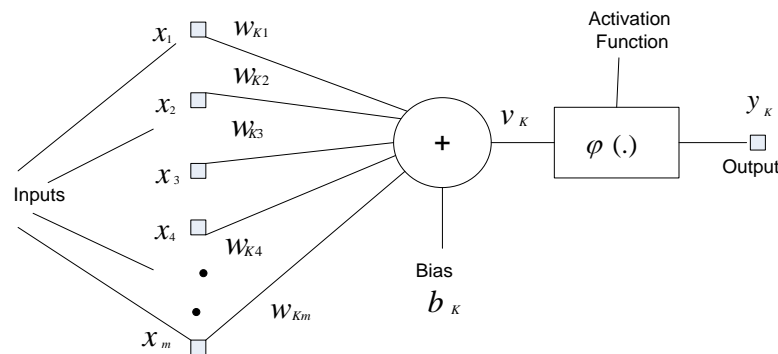


Figure 4. Typical model of ANN

The block diagram of the overall system of IM control with the proposed ANN speed estimator is shown in Figure 5. the ANN speed estimator consists of 3 layers (5- 10- 1). It has following structure, 5 inputs ( $V_{as}$ ,  $V_{\beta s}$ ,  $I_{as}$ ,  $I_{\beta s}$ ,  $\omega_r$ ) which are stationary voltages ( $V_{as}$ ,  $V_{\beta s}$ ) and current components of the stator ( $I_{as}$ ,  $I_{\beta s}$ ) as basic inputs and the reference speed ( $\omega_r$ ) is added as input to the ANN to increase its fitness, one hidden layer with 10 nodes, finally one output layer with single node which gives the estimated motor speed.

The selected ANN was designed and trained using MATLAB/Simulink and combined with the PI controller where, the activation function used is a sigmoid unipolar function, and Levenberge –Marquardt algorithm is applied in data training. The whole iterations number is 1000 epoch. From the training results; the mean square error is 0.0485 for PI controller as shown in Figure 6.



and the value of overshoot was added to the fitness function. The ITAE response for other case is shown in Figure 12, which also shows a good response than conventional-PI controller.

Table 1. IM nominal parameters	
Motor Parameter	Value
Output Power	0.75 kW, 3-ph
Speed	1440 rpm
Line voltage	220 V, Y-connected
Current	3 A
Frequency, f	50 Hz
Number of pair poles, P	2
$R_s, R_r$	6.37, 4.3 $\Omega$ respectively
$L_s, L_r, L_m$	0.26, 0.26, 0.24 H
Moment of inertia, J	0.0088 Kg.m <sup>2</sup>
B	0.003 Nm.s/rad

Table 2. PSO Parameters	
PSO Parameter	Value
Number of iterations	150
Number of particles	20
w	1.1
c1, c2	2
C	0.8

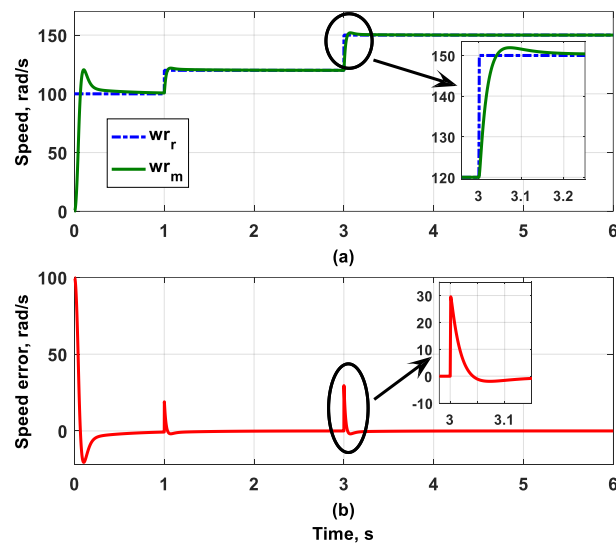


Figure 7. Reference speed step change with conventional PI controller, (a) Speed, (b) Speed error

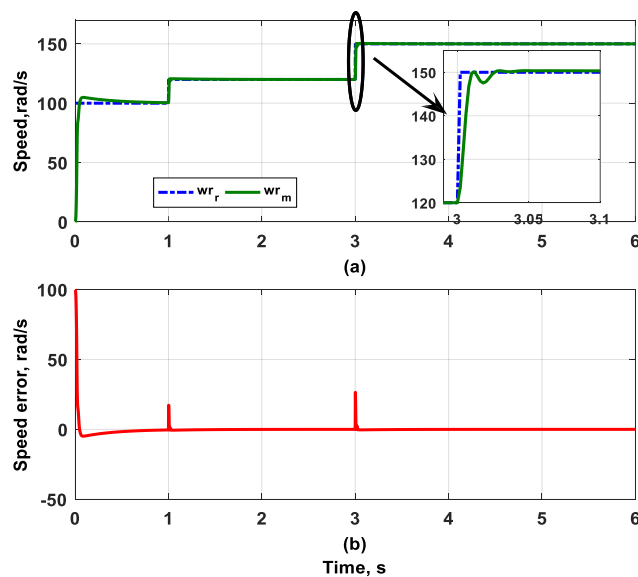


Figure 8. Reference speed step change with PSO-PI controller, (a) Speed, (b) Speed error

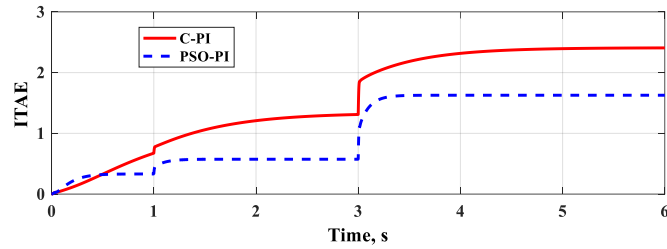


Figure 9. ITAE response for conventional and PSO-PI controller under step reference speed

For the second case the motor loading: the reference speed is changed in a trapezoidal way for studying the control system tracking performance for both directions also an external load with 5 Nm (nominal value) is applied between intervals 1.4s to 2.3s and between 3.9 s to 4.8s to study the robustness of the system under sudden applied loads. The results are better for PSO and the system is return to steady state quickly compared to the conventional PI controller.

Now the PSO-PI controller is tested for speed estimation with high speed command Figure 13 and low speed command which results is presented in Figure 14. By analyzing the last figures it's obvious that the suggested estimator has a valid response with different speed references. Figure 13 shows the increase of the speed reference starting from zero to 100rad/s gradually then step change to 15 rad/s and finally reduced to 75rad/s in all cases the system response is high and has a very small error between the actual speed and estimated one as shown in Figure 13 (c). the final case is the operating the system at low speed, Figure 14 in this case the reference speed is taken as a trapezoidal starting the motor operation at 0.6s with maximum speed value of 15rad/s. The figure shows that the system is still capable of working and track the reference speed at acceptable behavior.

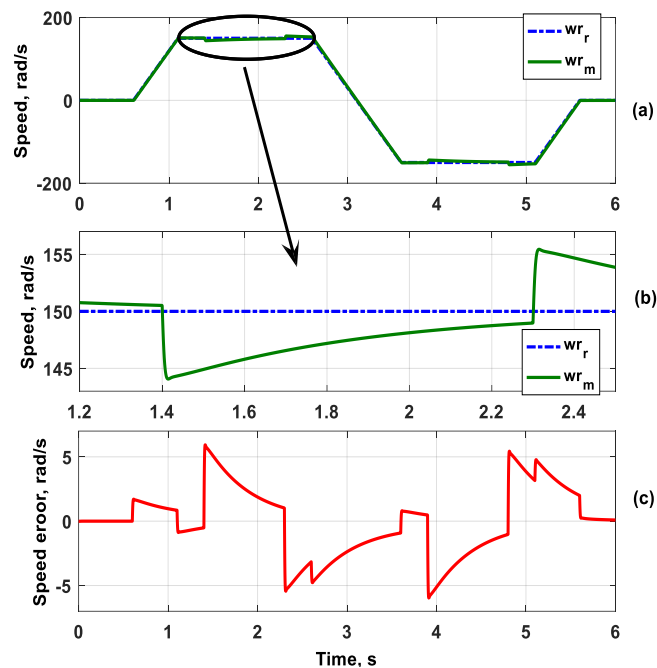


Figure 10. loading condition with conventional PI controller, (a) Speed response, (b) Focus on speed, (c) Speed error



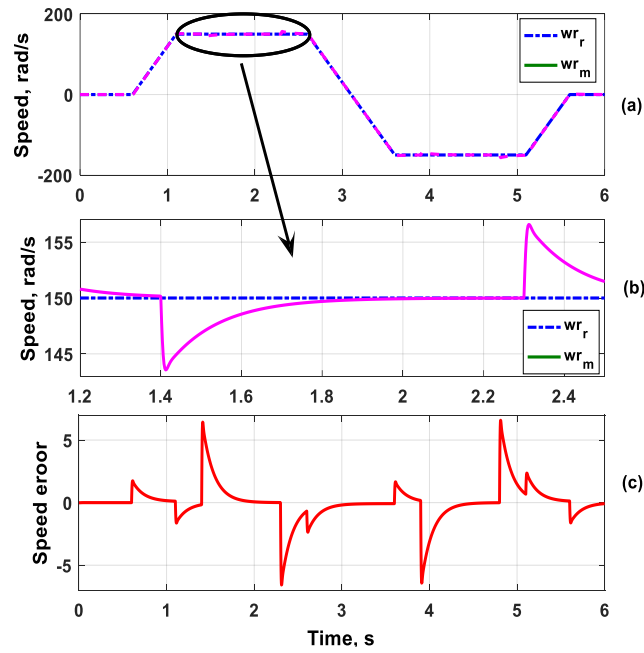


Figure11. loading condition with PSO-PI controller, (a) Speed response, (b) Focus on speed, (c) Speed error

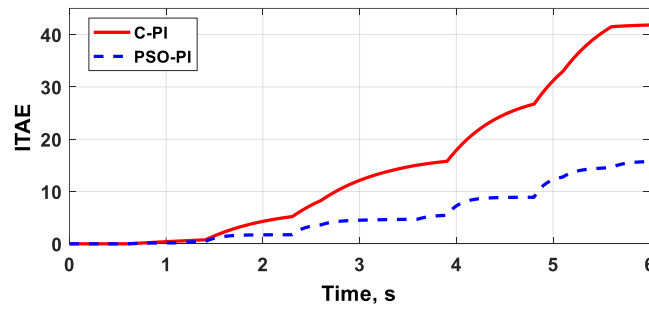


Figure12. ITAE response for conventional and PSO-PI controller under trapezoidal reference speed

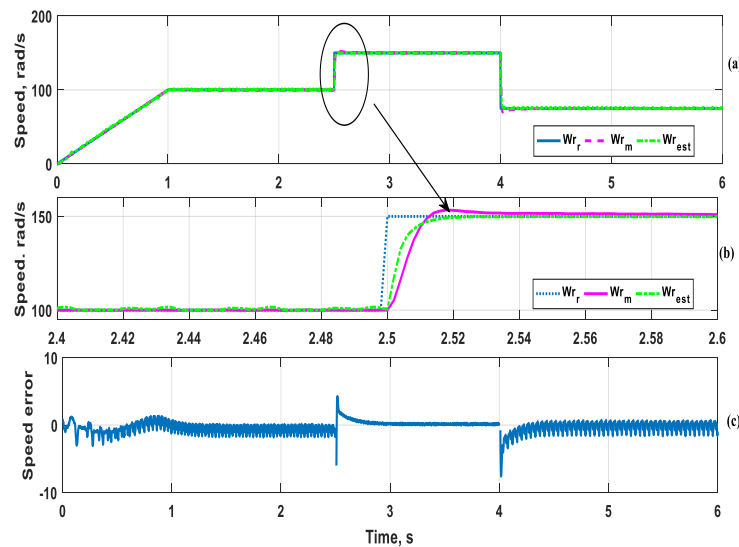


Figure 13. Step reference speed with PSO-PI controller; (a) Results for all simulated time, (b) Focus on the results, (c) Speed error

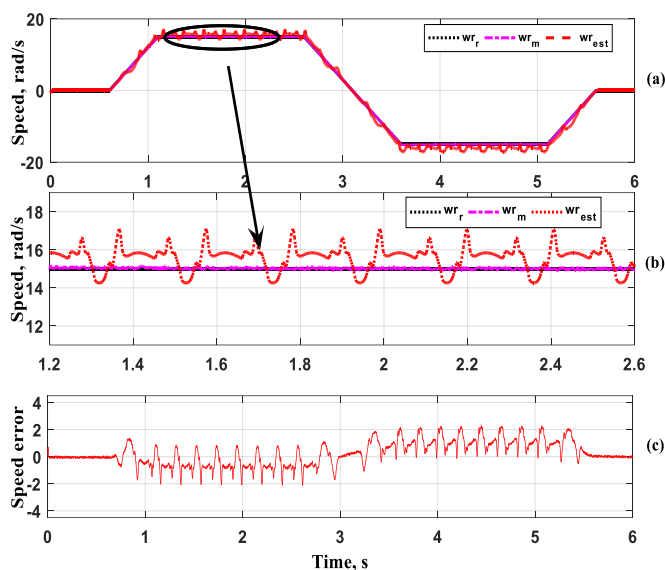


Figure14. Low speed condition with PI controller, (a) Results for all simulated time, (b) Focus on the results, (c) Speed error

## 6. CONCLUSION

This paper presented a proposed technique for IM speed control without speed sensor based IRFOC technique using FFNN as a speed estimator. The control technique was designed using PI controllers. The PI gains were tuned based on two different methods, the conventional and proposed method based on the PSO algorithm. The results were taken to compare the two methods. These results show that the proposed tuning method has good response comparing to the conventional method especially for step response where the overshoot was decreased to about 3% instead of 20% for the other one with decreasing the raising time and setting time. After that the speed estimator was designed based on the FFNN. The results were taken for various operating situations which show the efficiency for the sensorless technique especially at high speeds where the error was around 2% and has an acceptable value at low speed operations. The future work for this paper includes verifying of the proposed system using experimental validation and enhancing the speed estimation under very low speed operation.

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